

Understanding the Effects of Exponentially Decaying DC Currents on the Dual dq Control of Power Converters in Systems with High X/R

Daniel dos Santos Mota

Department of Electric Power Engineering
Norwegian University of Science and Technology
Trondheim, Norway
daniel.mota@ntnu.no

Elisabetta Tedeschi

Department of Electric Power Engineering
Norwegian University of Science and Technology
Trondheim, Norway
Department of Industrial Engineering
University of Trento
Trento, Italy
elisabetta.tedeschi@ntnu.no

Abstract—This paper investigates the root causes of detrimental oscillations in the dc link voltage of an energy storage system using a dual dq controller, operating at a high-voltage ac grid with high reactance-resistance ratio. Dual dq controllers are recommended in the literature for power converters operating under unbalanced, fault, or reduced voltage conditions. They employ two separated rotating reference frames, one for the positive and one for the negative sequence. The causes of the oscillations are investigated both theoretically and by time-domain computer simulations. As a result of the simulations, the performance of two dual controllers used in the industry is compared. In the presence of exponentially decaying dc currents, the filtering techniques employed by the controllers affect differently the performance of the proportional-integral regulators and disturb the feed forwarding and dq decoupling schemes. Ultimately, this results in undesirable oscillations in the dc-link voltage. This paper sheds light on how a fundamental phenomenon of three-phase ac systems can critically affect the control of power electronic converters. It provides a valuable insight into a possible root cause of oscillations in large electrical system applications with a considerable power converter penetration, such as large industrial plants striving for reducing greenhouse gas emissions.

Index Terms—power electronics, power systems, smart grids, renewable energies

I. INTRODUCTION

Offshore gas turbines responsible for heat and electricity generation in the oil and gas (O&G) fields on the Barents, North and Norwegian Seas account for roughly 20% of the total greenhouse gas (GHG) emissions of Norway [1]. In electrical engineering terms, the total installed capacity of the 150+ gas turbines on the Norwegian Continental Shelf (NCS) was approximately 3 GW with an yearly electrical

This research was funded by the Research Council of Norway through the PETROSENTER scheme, under the “Research Centre for Low-Emission Technology for Petroleum Activities on the Norwegian Continental Shelf” (LowEmission), grant number 296207.

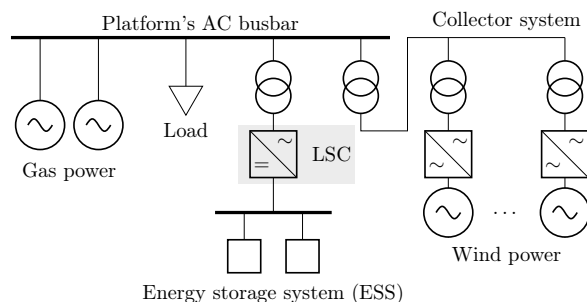


Fig. 1: Typical planned scenario for the electrical system of an O&G platform connected to an offshore wind farm.

energy consumption of 15 TWh in 2008 [2]. Although still at its infancy in a global scale, renewable offshore electricity generation is gaining momentum. Initiatives like the Hywind Tampen Project [3] point in the direction of a further increase in offshore wind electricity generation. Wind farms represent an extraordinary opportunity for reducing the offshore GHG emissions.

One typical planned scenario within this context is shown in Fig. 1. It illustrates a case study used by [4] of an O&G platform in the North Sea isolated from the continental electrical grid. This power intensive industrial process is fed by two 35 MW gas-powered generators. A techno-economical evaluation [5] suggests that a 12 MW offshore wind farm would be able to reduce the GHG emissions of this platform by 30%. For mitigating the effects of wind intermittency and for allowing the turbo-generators to operate at higher efficiency ranges, an energy storage system (ESS) would be connected directly to the main busbar of the platform. This paper uses the simplified, although realistic, model [6] of the case study depicted in Fig. 1 as base. See Table B.I in Appendix B for numerical data.

The reactance-resistance ratio (X/R) seen from the ac

terminals of the ESS's line side converter (LSC) towards the platform's busbar is high, as shown later in Section IV. Sudden changes in the voltage of three-phase systems with high X/R induce noticeable exponentially decaying dc currents. This phenomenon is well known among electrical engineers. However, in the authors' opinion, the time domain effects of these dc components in the control of power electronic converters are not covered in detail in the literature.

During the evaluation of different contingency scenarios for the case study depicted in Fig. 1, transient oscillations were detected in the voltage of the ESS's dc link. These oscillations were triggered by sudden changes to the busbar voltage and by sudden changes to the ESS's reactive or active power. The overall stability margin of the system was clearly reduced. The contingency scenario in question had the wind farm completely disconnected and the ESS's LSC operating with dual dq controllers. Such controllers work in two different rotating reference frames (RRFs), one specifically for positive sequence currents and voltages, and one for the negative sequence content. They were proposed in the literature as robust regulators for power converters operating in unbalanced three-phase systems [7, 8]. Moreover, they can also be activated in fault-ride through conditions with severe grid voltage drops [9].

In this article, the root causes of those oscillations are investigated and described. They are directly tied to the exponentially decaying dc currents of three-phase systems and to the way dual dq controllers split the positive and negative sequence measurements. Moreover, a comparison of the performance of two dual controller strategies is made via time-domain simulations. The first controller is the one proposed by [7] and later employed by authors closely linked to the industry [10, 11]. The other controller also stems from authors closely linked to the industry [8, 12, 13].

The theoretical insights obtained from this study can benefit not only engineers working with the integration of renewable energies into O&G platforms, but also those working with converter interfaced renewable energy sources in general, specially those related to island and country-wide electrical grids.

II. CONTROL IN A ROTATING REFERENCE FRAME

The power converter analyzed in this paper is the ESS's LSC of Fig. 1. The control of this converter is performed on a RRF which allows the use of proportional and integral (PI) regulators [14]. This is also known as vector control in the industry. It relies on $abc \mapsto dq$ and $dq \mapsto abc$ transformations. A comprehensive explanation on the history of these transformations, on their different variants, and on their geometrical foundations is given by [15]. See Appendix A for a list of the transformations used throughout the paper.

Let the LSC and gas-powered generators of the platform be modeled as two ideal voltage sources interconnected by a resistive and inductive (RL) impedance. Equation (1) shows the relationship between the voltages and currents in this circuit moved to the dq_+ with (A.2) and (A.3). The voltages

of the converter are denoted by v_c , whereas the generator voltage is denoted by v_g . The generic term grid voltage will be employed from now on when referring to v_g . A strong coupling between the d and q axes is evident.

$$\begin{bmatrix} v_{gd} \\ v_{gq} \end{bmatrix} + R \begin{bmatrix} i_d \\ i_q \end{bmatrix} + \omega L \begin{bmatrix} 0 & -1 \\ 1 & 0 \end{bmatrix} \begin{bmatrix} i_d \\ i_q \end{bmatrix} + L \frac{d}{dt} \begin{bmatrix} i_d \\ i_q \end{bmatrix} = \begin{bmatrix} v_{cd} \\ v_{cq} \end{bmatrix} \quad (1)$$

Equation (2) shows how the current in (1) can be controlled in the dq_+ frame. The influence of the non-controllable grid voltage is canceled by summing it to the output of the PI controller. This is known as feed forwarding. The decoupling of the dq axes is obtained with the $\omega' L i'$ term. The matrix in this term is named decoupling matrix \mathbf{M} .

$$\begin{bmatrix} v_{cd} \\ v_{cq} \end{bmatrix} = \begin{bmatrix} v_{cdPI} \\ v_{cqPI} \end{bmatrix} + \begin{bmatrix} v'_{gd} \\ v'_{gq} \end{bmatrix} + \omega' L \begin{bmatrix} 0 & -1 \\ 1 & 0 \end{bmatrix} \begin{bmatrix} i'_d \\ i'_q \end{bmatrix} \quad (2)$$

Assuming the feed forwarding and decoupling work perfectly, this multiple-input multiple-output (MIMO) system becomes two independent single-input single-output (SISO) systems. The Modulus Optimum tuning technique [16] with the modifications recommended by [17] is well suited for tuning these controllers.

It is worth remarking that the currents on (1) are representations of the actual quantities in the process, whereas the currents on (2) are measurements inside the controller. The same applies to the voltages and to the angular frequency. Therefore, these measurements are denoted by v'_g , ω' , and i' in (2). Attenuation and phase shifts introduced by filtering degrade the performance of the PI regulators and can, potentially, disrupt the feed forwarding and the decoupling schemes during transients.

III. DUAL dq CONTROLLERS

Dual dq controllers were proposed in the literature as robust regulators for power electronic converters working under unbalanced and distorted conditions [7, 8]. They operate in two independent dq reference frames, a dq_+ for the positive sequence and a dq_- for the negative sequence, as shown in Fig. 2. A generic positive sequence measurement in the abc frame with fixed amplitude and fixed phase lag φ becomes dc when moved to dq_+ with the transformation (A.2). Conversely, a negative sequence measurement moved to the dq_+ frame becomes second harmonic. For that reason, dual controllers rely on filtering the second harmonic for removing the negative sequence content from the dq_+ frame. Dually, in the dq_- frame, the positive sequence content becomes second harmonic and needs, thus, to be removed by filtering.

A. Notch-Based Dual dq Controller

In 1999, a dual control scheme was proposed by [7]. The positive sequence RRF is the aforementioned dq_+ . However, the authors changed the sign of ω in the Park transformation (rotation from $\alpha\beta$ to dq) for representing the negative sequence RRF. For that reason, this frame is named $dq_{-\omega}$ in this paper. The transformation between frames uses the matrices (A.1) and (A.5) from the Appendix A. Moreover, all references to

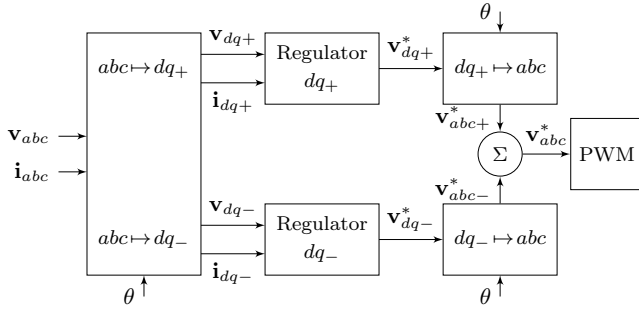


Fig. 2: Dual dq controller.

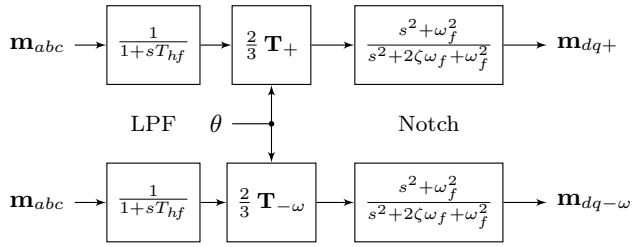


Fig. 3: Notch-filter-based transducer for the positive sequence and negative ω RRFs, adapted from [7, 9, 10, 18]; the measurements \mathbf{m} stand for either voltages or currents.

dq_- in Fig. 2 should be understood as $dq_{-\omega}$ for this dual controller.

A notch filter tuned to the second harmonic removes the opposite sequence measurements from each of the dq frames. For this reason, this dual controller is named “notch-based” in this paper. A low-pass filter (LPF) with a cutout frequency tuned to 1000 Hz is added for signal conditioning at the inputs [9]. Fig. 3 shows an adaptation of the dual positive and negative ω RRF transducer used by [7], and further discussed by [9, 10, 18]. Attention must be paid when building the negative ω RRF controller as the signs of the decoupling matrix \mathbf{M} of (2) are inverted in the different RRFs. This fact is illustrated on [7, 9, 18].

The damping factor ζ in Fig. 3 defines the quality of the filter. The lower the damping, the higher the quality, i.e., lower attenuation and lower phase shifts outside the notch frequency. Nevertheless, this comes at the cost of complex conjugated poles with increasingly lower damping [19]. Computer simulations with $\zeta = \sqrt{2}/2$ showed good results. However, for a fair comparison with the other dual controller, a unitary ζ is chosen.

B. LPF-Based Dual dq Controller

In 2012, [8] proposed a dual dq controller based on [20]. The two RRFs in this controller are a positive sequence dq_+ and a negative sequence dq_- , see (A.1) and (A.4). It is worth noting that the decoupling matrix \mathbf{M} of (2) can be directly used in the dq_- frame. This can be verified by using the matrices

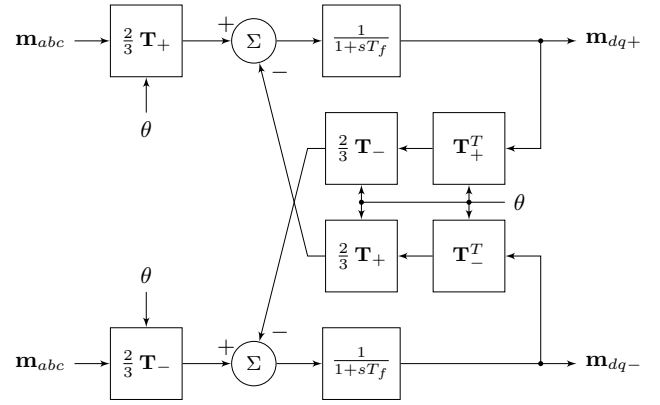


Fig. 4: LPF-based transducer for positive and negative sequence RRFs, adapted from [20]; the measurements \mathbf{m} stand for either voltages or currents.

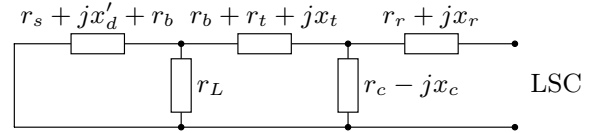


Fig. 5: Single-line diagram used for the X/R calculation.

in the Appendix A to re-write the quantities of (1) into the dq_- frame.

The measurement principles of the dual controller proposed by [8] rely on LPFs as shown in Fig. 4. For that reason, the controller is denoted as “LPF-based” in this paper. The measurements \mathbf{m}_{dq+} and \mathbf{m}_{dq-} are the outputs of LPFs. They are transformed back to the other RRFs and become second harmonic. At the summation blocks, they cancel the undesirable opposite sequence content from each RRF.

According to [20], the cutout frequency of the LPFs should be lower or equal to $f_n/\sqrt{2}$, where f_n is the fundamental, for guaranteeing a stable and damped response of the transducer. The cutout frequency is, in this paper, set to $f_n/\sqrt{2}$.

IV. ESTABLISHING A REPRESENTATIVE RANGE OF X/R

It is now time to set the dual controllers within the high X/R scenario depicted in Fig. 1. The reactance-resistance ratio in question in this paper is the one seen from the ac terminals of the ESS’s LSC towards the platform’s busbar. In this section, a representative range of values for X/R is determined. Fig. 5 summarizes this calculation.

As previously mentioned, the wind farm transformer at the platform is disconnected from the busbar. The two synchronous generators are modeled as a voltage source behind the transient reactance x'_d in series with the stator resistance r_s . The resistance r_b represents the losses in the circuit breaker and other high-voltage (HV) devices. The load is simplified as a fixed resistor r_L . Typical short-circuit impedance and full load losses taken from [21] are used to derive x_t and r_t of the ESS’s transformer. Moreover, x_t is adopted as the line-side

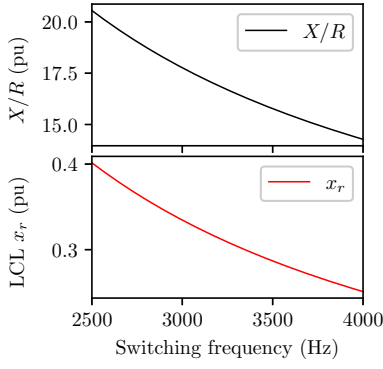


Fig. 6: Representative range of X/R and LCL converter-side reactance versus PWM switching frequency for the scenario in Fig. 1 with the wind farm disconnected.

reactance of the converter's inductor-capacitor-inductor (LCL) filter. See Tables B.I and B.II in Appendix B for numerical values.

The main contributor to the X/R seen from the LSC's ac terminals is the converter-side reactor of the LCL filter, x_r in Fig. 5. For MW-sized converters like the ones in [22], paralleled two-level insulated-gate bipolar transistor (IGBT) bridges with individual LCL filters are typically employed. Without losing generality for estimating the range of X/R , the LSC can be modeled as one single converter with one single LCL.

The design of LCL filters is well documented in the literature [23–26]. In this paper, the criteria described by [26] are used for calculating the reactances x_r and x_c and the resistance r_c in Fig. 5. Those depend on the pulse-width modulation (PWM) switching frequency f_{sw} and on the dc link's rated voltage. For MW-sized converters such as the ones in [27], f_{sw} can be selected between 1 kHz and 4 kHz. Fig. 6 shows a representative range of values for X/R and for the calculated values of x_r as a function of the PWM switching frequency.

V. EXPONENTIALLY DECAYING DC CURRENTS IN THREE-PHASE SYSTEMS

The impedance seen from the ac terminals of the ESS's LSC in Fig. 1 has an X/R on the range of 10 to 20. Sudden changes at the voltage of the LSC induce exponentially decaying dc currents with a transient time (3τ) between 80 ms to 160 ms. For understanding the effects of exponentially decaying dc currents on the control of power converters, it is important to recapitulate a few basic principles.

If a positive-sequence three-phase voltage source with amplitude V is connected to a RL load, the current supplied to each phase of the load is

$$i(t) = \frac{V}{\|Z\|} \left[-e^{-t/\tau} \sin(\gamma - \varphi) + \sin(\omega t + \gamma - \varphi) \right] \quad (3)$$

where $\varphi = \arctan(\omega L/R)$, $\|Z\| = \sqrt{(\omega L)^2 + R^2}$, and γ is the initial phase of the voltage, i.e., zero, or $-2\pi/3$, or $+2\pi/3$.

The currents in (3) can be split into exponentially decaying and sinusoidal components. The latter form a positive sequence in response to the feeding voltage. The former, on the other hand, are neither positive nor negative sequence. There is no sinusoidal variation with time. They do not contribute to zero sequence either as their sum is continuously equal to zero. Equation (4) shows the three-phase exponentially decaying current components organized as a vector.

$$\mathbf{i}_{\text{exp}} = \frac{V}{\|Z\|} e^{-t/\tau} \begin{bmatrix} \sin(\varphi) \\ \sin(\varphi + 2\pi/3) \\ \sin(\varphi - 2\pi/3) \end{bmatrix} \quad (4)$$

A. Positive Sequence RRF

Equation (5) shows (4) moved into the positive sequence RRF. The exponentially decaying dc currents in the abc frame become an exponentially decaying fundamental in dq_+ .

$$\mathbf{i}_{\text{exp}_{dq_+}}(t) = \frac{2\mathbf{T}_+}{3} \mathbf{i}_{\text{exp}}(t) = \frac{V e^{-t/\tau}}{\|Z\|} \begin{bmatrix} -\cos(\omega t + \varphi) \\ \sin(\omega t + \varphi) \end{bmatrix} \quad (5)$$

The instantaneous power supplied to a three-phase circuit is given by (6). The power dissipated by the currents in (5) can be calculated with (6), resulting in (7).

$$p(t) = \begin{bmatrix} v_a(t) \\ v_b(t) \\ v_c(t) \end{bmatrix}^T \begin{bmatrix} i_a(t) \\ i_b(t) \\ i_c(t) \end{bmatrix} = \frac{3}{2} [v_d(t) \quad v_q(t)] \begin{bmatrix} i_d(t) \\ i_q(t) \end{bmatrix} \quad (6)$$

$$p(t) = -\frac{3}{2} \frac{V^2}{\|Z\|} e^{-t/\tau} \cos(\omega t + \varphi) \quad (7)$$

The transient dc currents in the abc frame cause an oscillation in the instantaneous power delivered by the voltage source to the load. Active power oscillations directly affect the dc-link voltage of the converter. If a dual controller is expected to dampen exponentially decaying dc components in the abc frame, it should preserve the fundamental frequency components of the measurements in the dq frame. However, for a dual controller to work, it needs to filter out the second harmonic from its dq frames. Unfortunately, both tasks cannot be perfectly achieved with zero attenuation and phase shift with causal filters [18].

B. Negative Sequence RRF

The LPF-based controller uses the negative sequence dq_- frame. Equation (8) shows (4) moved to dq_- with (A.4). The exponentially decaying dc currents in the abc frame appear as exponentially decaying fundamental in dq_- .

$$\mathbf{i}_{\text{exp}_{dq_-}}(t) = \frac{2\mathbf{T}_-}{3} \mathbf{i}_{\text{exp}}(t) = \frac{V e^{-t/\tau}}{\|Z\|} \begin{bmatrix} \cos(\omega t - \varphi) \\ -\sin(\omega t - \varphi) \end{bmatrix} \quad (8)$$

C. Negative ω RRF

The notch-based dual controller uses a negative ω RRF, see Appendix A. Equation (9) shows (4) moved to the $dq_{-\omega}$ frame.

$$\mathbf{i}_{\text{exp}_{dq_{-\omega}}}(t) = \frac{2\mathbf{T}_{-\omega}}{3} \mathbf{i}_{\text{exp}}(t) = \frac{V e^{-t/\tau}}{\|Z\|} \begin{bmatrix} -\cos(\omega t - \varphi) \\ -\sin(\omega t - \varphi) \end{bmatrix} \quad (9)$$

Notice that direct quantities in $dq_{-\omega}$ feature the opposite sign of the ones in the dq_{-} frame. The quadrature quantities, on the other hand, have the same sign. This has to be taken into consideration when comparing the two types of dual controllers.

VI. COMPARING THE MEASUREMENT PRINCIPLES OF THE DUAL dq CONTROLLERS

The positive and negative sequence measurement principles of the notch-based and the LPF-based dual controllers are compared in this section. This is done by simulating the connection of a three-phase positive-sequence voltage source to an RL load. The voltage amplitude is set to 0.1 pu, the frequency to 60 Hz, the reactance to 0.5 pu, and the resistance to 0.025 pu. The angular frequency measurement is assumed to be instantaneous. Moreover, zero delay is assumed for the measurement of θ in Fig. 2.

The currents in the dq frames can be analytically determined with (3) and the transformation matrices of the Appendix A. The reactance-resistance ratio is at the highest representative range for the scenario analyzed in this paper. This highlights the effects of the exponentially decaying dc components without reducing the generality of the results. It is necessary to remark that the direct negative sequence measurements (d_{-}) of the LPF-based dual controller are multiplied by -1 in all figures for allowing a direct comparison with the notch-based principle.

Fig. 7a shows the dq_{+} voltage measured by the notch and the LPF-based measuring principles. The response for v_{d+} is similar for both principles except for the second order characteristics on the notch-based measurement. The notch-based transducer measures the expected value of $v_{q+} = 0$ pu. However, the cross-coupling of RRFs of the LPF-based principle (see Fig. 4) shows its influence. A deviation of almost 0.02 pu is observed in the v_{q+} measured by the LPF-based transducer after the 0.1 pu change in the positive-sequence voltage.

Fig. 7c shows dq_{-} and $dq_{-\omega}$ measurements with the notch and the LPF-based measuring principles. Although featuring a sharper increase at the beginning, the measurements in both direct and quadrature axes with the notch-based principle return to zero faster than the measurements with the LPF-based transducer.

Figs. 7b and 7d show the measurements of the currents in the dq_{+} , dq_{-} , and $dq_{-\omega}$ frames. In all cases, the phase shifts featured by the LPF-based transducer are larger than the ones featured by the notch-based. This is an indication that the performance of the PI regulators, as well as the decoupling of the dq axes will be worse for the LPF-based dual controller. Moreover, this also indicates that the notch-based dual controller will have a better overall performance during transients than its counterpart.

VII. COMPARING THE PERFORMANCE OF THE DUAL dq CONTROLLERS

In this section, the performance of the notch-based and LPF-based dual controllers employed at a scenario with high

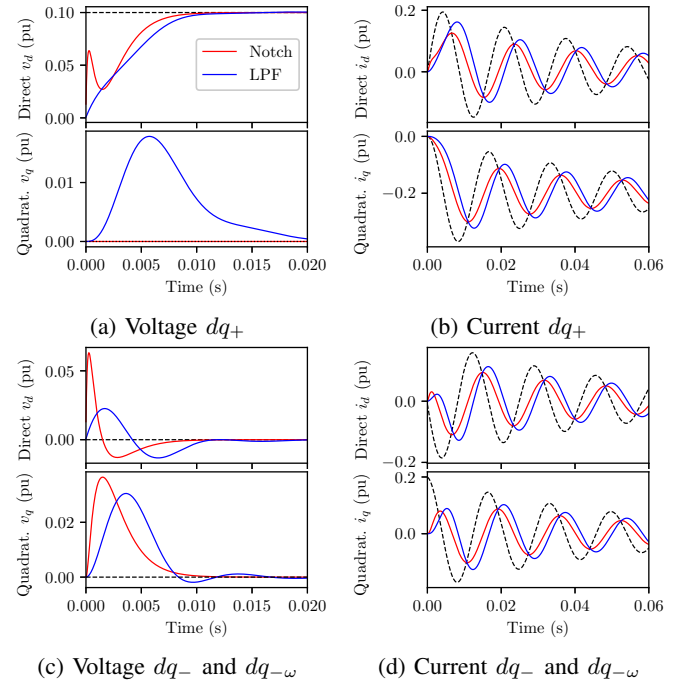


Fig. 7: Comparison of the measurement principles; notch-based in red, LPF-based in blue, ideal measurements in dashed black.

X/R as the one in Fig. 1 are evaluated. This is done by simulating a controlled voltage source representing the LSC connected to the grid via a reactance in series with a resistance. Initially, the grid voltage is a pure positive sequence with 1 pu amplitude. The reactance and resistance are the same as the ones employed in Section VI. All PI regulators have the structure $K(1+sT)/(sT)$. They are tuned equally in both dual controllers. The integrator time is adjusted to $Ti = X/(\omega R)$, whereas the proportional gain K is set to 4 (see Section II).

In the first two tests shown, all current references are set to zero. Therefore, deviations from zero in the currents and instantaneous power are key performance indicators. The higher the deviations and the longer their duration, the worse the performance. For the last test, however, a step is applied to the reference of the positive sequence quadrature current which results in a pure reactive current. The active power dissipated by this current is equal to 0.001 pu and can be treated, for all practical purposes, as zero in this comparison. For the pu bases, see Table B.I.

Fig. 8a shows the response of the notch-based regulator to an instantaneous 0.2 pu drop at the grid voltage at $t = 0.5$ s. The feed forwarding of the grid voltage works quickly, resulting in almost instantaneous changes to the converter voltage. The exponentially decaying currents induced by the sudden change in the grid voltage are not easily discernible. The notch-based regulator brings the currents back to zero in less than 50 ms. There is a small perturbation in the active power which goes over 0.01 pu for approximately 10 ms. For the LPF-based dual controller, Fig. 8b, the feed forwarding is

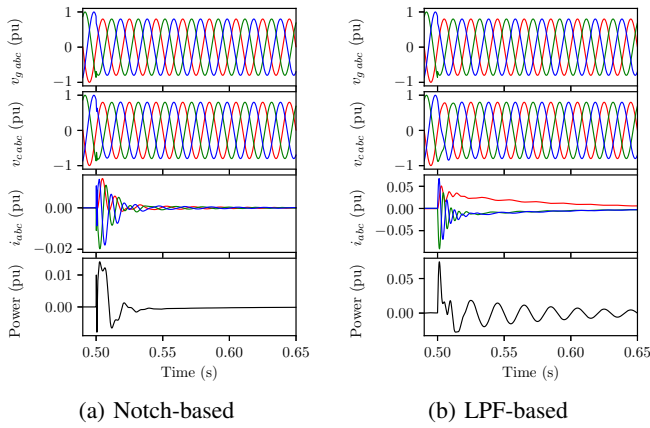


Fig. 8: Response to a drop in the grid voltage, positive sequence only; phase a in red, b in green, c in blue, and instantaneous power in black.

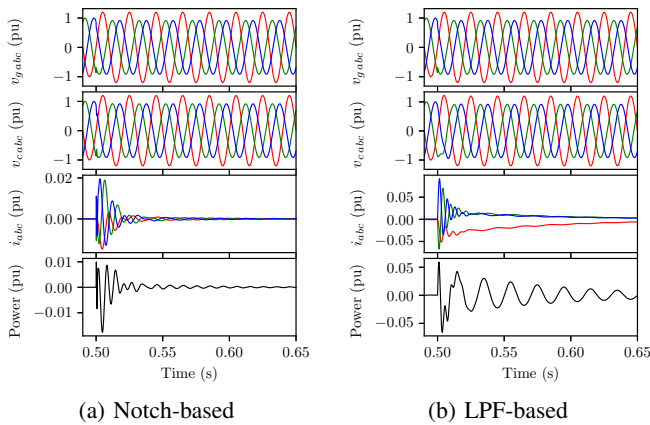


Fig. 9: Response to a step at the grid voltage negative sequence content; phase a in red, b in green, c in blue, and instantaneous power in black.

not as fast as for the notch-based one. The transitions in the converter voltage right after $t = 0.5$ s are smoother. Moreover, the instantaneous power for the LPF-based controller peaks at 0.074 pu and, later, oscillates with 60 Hz for more than 150 ms. This is due to the slow decay of the dc components of the current.

Fig. 9a shows the response of the notch-based regulator to a sudden introduction of a negative sequence with 0.2 pu amplitude at $t = 0.5$ s. The notch-based regulator manages to bring the currents back to zero within 50 ms, whereas the LPF-based one does not (Fig. 9b). Similarly to the previous results with the LPF-based controller, the decay of the dc components in the current is slow causing the instantaneous power to oscillate with 60 Hz.

Fig. 10 shows the last tests performed with the dual controllers. A step of -0.2 pu is applied at the positive sequence quadrature current reference at $t = 0.5$ s. A remarkable difference between the converters response is the time it takes for them to achieve a balanced supply of current. The notch-

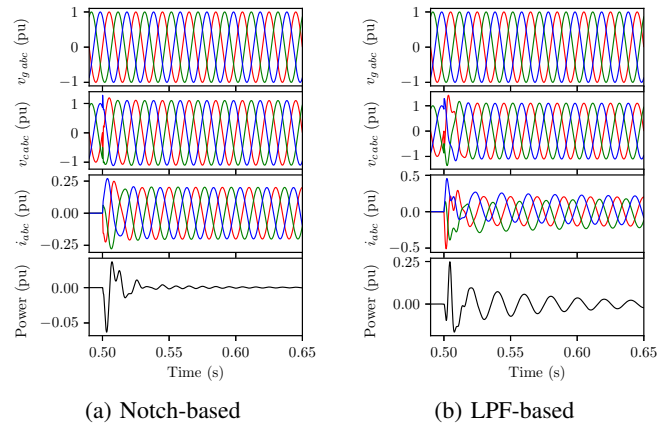


Fig. 10: Response to step at the i_{q+} reference; phase a in red, b in green, c in blue, and instantaneous power in black.

TABLE I: Comparison of the performance of the dual controllers; the higher Δp the worse; 1 pu = 9.65 MW.

Test	Notch-based	LPF-based
	Max. Δp pu	Max. Δp pu
Pos. seq. grid volt. drop of 0.2 pu	0.014	0.074
Neg. seq. step -0.2 pu at grid voltage	0.018	0.066
Step at the reference of i_{q+}	0.036	0.249

based controller manages it within 30 ms, whereas the LPF-based takes more than 150 ms.

The overall performance of the notch-based regulator is better than the one of the LPF-based, see Table I. The notch-based is able to dampen the dc current components in less than the expected transient time $3\tau = 160$ ms, being the components caused by uncontrolled grid voltage changes (Figs. 8 and 9) or caused by controlled LSC voltage changes (Fig. 10). The LPF-based, on the other hand, has a much worse performance. The larger phase shifts in the measurements (Fig. 7) make the feed forwarding of the grid voltage slower and, in addition, degrade the response of the PI regulators with their decoupling scheme.

VIII. CONCLUSIONS

This paper investigated the root causes of undesired transient oscillations in the dc link of an ESS using a dual dq controller in an electrical system with high X/R .

Dual dq controllers were proposed in the literature as robust regulators for power electronic converters operating under unbalanced and distorted conditions. They work in two RRFs and rely on filtering the second harmonic from the measurements in the dq frame for correctly isolating the positive from the negative sequence content.

Sudden changes to the voltage of three-phase electrical systems with high X/R induce exponentially decaying dc currents in the abc frame. These currents become exponentially decaying sinusoidal signals with the fundamental frequency when moved to the dq frame. They need to be properly

measured if a controller is to dampen them. Dual dq controllers are thus faced with two conflicting tasks to be performed concurrently in their dq frames: 1) remove the second harmonic to split positive and negative sequences; and 2) preserve the fundamental frequency components of the measurements.

As a part of the investigations on the root causes of the oscillations in the dc link of the ESS of Fig. 1, the performance of two dual dq controllers were compared. The simulations on a conceptual model presented in Section VII showed that the dual controllers are stable, albeit with different dynamic responses in spite of the identical tuning of the PI regulators. The notch-based controller handled transients considerably better than the LPF-based did. From the response to the step at the quadrature current reference, it is possible to infer that, for the same proportional gain, the LPF-based controller is less stable than the notch-based.

The filtering techniques necessary for a dual dq controller to work introduce phase shifts to the measurement of the exponentially decaying currents. In addition to degrading the performance of the PI regulators, these phase shifts also delay the feed forwarding of the grid voltage and perturb the decoupling of the dq axes during transients. This results in noticeable oscillations in the active power exchange between converter and grid, which, ultimately, manifest themselves as undesirable transient oscillations in the dc-link voltage.

The analysis of the problem in the time-domain, with focus on the effects of exponentially decaying dc currents in three-phase systems with high X/R in the dual dq control of power electronic converters is the main contribution of this paper. It provides a valuable insight into a possible root cause of oscillations in high capacity power converters operating in large electrical systems, being them isolated O&G platforms or country-wide grids.

REFERENCES

- [1] *Norsk Petroleum Emissions to Air*. Norwegianpetroleum.no. Feb. 17, 2020. URL: <https://www.norskpetroleum.no/en/environment-and-technology/emissions-to-air/> (visited on 02/17/2020).
- [2] *Kraft fra land til norsk sokkel*. Technical Report. Norway: Oljedirektoratet, Norges vassdrags og energidirektorat, Petroleumtilsynet, Statens forurensningstilsyn, Jan. 2008, p. 99. URL: <https://www.npd.no/globalassets/1-mpd/publikasjoner/rapporter/kraft-fra-land-rapport.pdf> (visited on 04/21/2021).
- [3] *Hywind Tampen - Floating Wind Power Project - Equinor.Com*. Hywind Tampen: the world's first renewable power for offshore oil and gas. Mar. 3, 2020. URL: <https://www.equinor.com/en/what-we-do/hywind-tampen.html> (visited on 04/19/2021).
- [4] E. F. Alves, D. d. S. Mota, and E. Tedeschi. "Sizing of Hybrid Energy Storage Systems for Inertial and Primary Frequency Control". In: *Unpublished* (2021).
- [5] L. Riboldi et al. "Innovative Hybrid Energy System for Stable Power and Heat Supply in Offshore Oil & Gas Installation (HES-OFF): System Design and Grid Stability". In: ed. by S. Pierucci et al. Vol. 48. 30 European Symposium on Computer Aided Process Engineering. Elsevier, Jan. 1, 2020, pp. 211–216. DOI: 10.1016/B978-0-12-823377-1.50036-7.
- [6] E. F. Alves. *Efantnu/Hybrid-Ess-Design: Review 1 Release*. Zenodo, Mar. 12, 2021. DOI: 10.5281/zenodo.4601067. URL: <https://zenodo.org/record/4601067#.YHoHlegzaUk> (visited on 04/16/2021).
- [7] H. S. Song and K. Nam. "Dual Current Control Scheme for PWM Converter under Unbalanced Input Voltage Conditions". In: *IEEE Transactions on Industrial Electronics* 46.5 (Oct. 1999), pp. 953–959. ISSN: 1557-9948. DOI: 10.1109/41.793344.
- [8] D. Siemaszko. "Positive and Negative Sequence Control for Power Converters under Weak Unbalanced Networks". In: *Railway and Ship Propulsion 2012 Electrical Systems for Aircraft*. Oct. 2012, pp. 1–6. DOI: 10.1109/ESARS.2012.6387479.
- [9] J. B. Glasdam. *Harmonics in Offshore Wind Power Plants: Application of Power Electronic Devices in Transmission Systems*. Springer, Oct. 26, 2015. 219 pp. ISBN: 978-3-319-26476-9.
- [10] P. Brogan. "The Stability of Multiple, High Power, Active Front End Voltage Sourced Converters When Connected to Wind Farm Collector Systems". In: *EPE Wind Energy Chapter Seminar*. Stafford, 2010.
- [11] P. B. Brogan et al. "Improved Converter Network Bridge Controller". U.S. pat. 20210021209A1. Jan. 21, 2021. URL: <https://uspto.report/patent/app/20210021209> (visited on 04/16/2021).
- [12] D. Siemaszko. "Double Frame Control and Power Compensation for Power Converters Connected to Weak Networks with Disturbances". In: 2013 15th European Conference on Power Electronics and Applications (EPE). Sept. 2013, pp. 1–10. DOI: 10.1109/EPE.2013.6631736.
- [13] D. Siemaszko and A. C. Rufer. "Power Compensation Approach and Double Frame Control for Grid Connected Converters". In: 2013 IEEE 10th International Conference on Power Electronics and Drive Systems (PEDS). Apr. 2013, pp. 1263–1268. DOI: 10.1109/PEDS.2013.6527213.
- [14] F. Blaabjerg et al. "Overview of Control and Grid Synchronization for Distributed Power Generation Systems". In: *IEEE Transactions on Industrial Electronics* 53.5 (Oct. 2006), pp. 1398–1409. ISSN: 1557-9948. DOI: 10.1109/TIE.2006.881997.
- [15] C. J. O'Rourke et al. "A Geometric Interpretation of Reference Frames and Transformations: Dq0, Clarke, and Park". In: *IEEE Transactions on Energy Conversion* 34.4 (Dec. 2019), pp. 2070–2083. ISSN: 1558-0059. DOI: 10.1109/TEC.2019.2941175.
- [16] F. Fröhr and F. Ortenburger. *Introduction to Electronic Control Engineering*. Berlin and München, Germany; London, UK: Siemens Aktiengesellschaft; Heyden & Son LTD., 1982. ISBN: 0-85501-290-0.
- [17] J. A. Suul et al. "Tuning of Control Loops for Grid Connected Voltage Source Converters". In: 2008 IEEE 2nd International Power and Energy Conference. Dec. 2008, pp. 797–802. DOI: 10.1109/PECON.2008.4762584.
- [18] L. H. Kocewiak. *Harmonics in Large Offshore Wind Farms*. Department of Energy Technology, Aalborg University, Denmark, 2012. ISBN: 978-87-92846-04-4.
- [19] Z. Ye and H. Mohamadian. "Application of Modern Control Theory on Performance Analysis of Generalized Notch Filters". In: 2016 5th International Conference on Modern Circuits and Systems Technologies (MOCASST). May 2016, pp. 1–4. DOI: 10.1109/MOCASST.2016.7495100.
- [20] P. Rodriguez et al. "Decoupled Double Synchronous Reference Frame PLL for Power Converters Control". In: *IEEE Transactions on Power Electronics* 22.2 (Mar. 2007), pp. 584–592. ISSN: 1941-0107. DOI: 10.1109/TPEL.2006.890000.
- [21] *GFAFOL Cast-Resin Transformers 100 to 16,000 kVA*. Catalogue TV1—2013. Erlangen, Germany: Siemens AG, 2013.
- [22] *ACS880-77LC/-87LC/-87CC Wind Turbine Converters*. System Description 3AXD50000022022 Rev C. ABB, Apr. 27, 2020. URL: <https://search.abb.com/library/Download.aspx?DocumentID=3AXD50000022022&LanguageCode=en&DocumentPartId=1&Action=Launch> (visited on 06/26/2020).
- [23] M. Liserre, F. Blaabjerg, and A. Dell'Aquila. "Step-by-Step Design Procedure for a Grid-Connected Three-Phase PWM Voltage Source Converter". In: *International Journal of Electronics* 91.8 (Aug. 1, 2004), pp. 445–460. ISSN: 0020-7217. DOI: 10.1080/00207210412331306186.
- [24] R. Peña-Alzola et al. "Analysis of the Passive Damping Losses in LCL-Filter-Based Grid Converters". In: *IEEE Transactions on Power Electronics* 28.6 (June 2013), pp. 2642–2646. ISSN: 1941-0107. DOI: 10.1109/TPEL.2012.2222931.
- [25] R. N. Beres et al. "A Review of Passive Power Filters for Three-Phase Grid-Connected Voltage-Source Converters". In: *IEEE Journal of Emerging and Selected Topics in Power Electronics* 4.1 (Mar. 2016), pp. 54–69. ISSN: 2168-6785. DOI: 10.1109/JESTPE.2015.2507203.
- [26] H. Brantsæter et al. "Passive Filter Design and Offshore Wind Turbine Modelling for System Level Harmonic Studies". In: *Energy Procedia*

- [27] *The Top-Performing Wind Converter Trusted Technology for Maximum Power Yield – SINAMICS W180*. Brochure PDL-D-B10099-00-7600. Siemens AG, 2017. URL: https://assets.new.siemens.com/siemens/assets/api/uuid:26ef63b7cae9657fae9e98618212ba874f3fd729/455_170680_ws_sinamicw180us.pdf (visited on 09/27/2020).

APPENDIX A

REFERENCE FRAMES AND TRANSFORMATIONS

A. Positive Sequence Rotating Reference Frame

Equation (A.1) shows the matrix \mathbf{T}_+ used in the $abc \mapsto dq_+$ and $dq_+ \mapsto abc$ transformations. The power converters analyzed in this study are connected to the grid via an ungrounded delta-wye transformer. Therefore, the zero sequence is disregarded.

$$\mathbf{T}_+ = \begin{bmatrix} \sin(\omega t) & \sin(\omega t - 2\pi/3) & \sin(\omega t + 2\pi/3) \\ \cos(\omega t) & \cos(\omega t - 2\pi/3) & \cos(\omega t + 2\pi/3) \end{bmatrix} \quad (\text{A.1})$$

The $abc \rightarrow dq_+$ transformation is given by (A.2).

$$\begin{bmatrix} m_d(t) \\ m_q(t) \end{bmatrix} = \frac{2}{3} \mathbf{T}_+(t) \begin{bmatrix} m_a(t) \\ m_b(t) \\ m_c(t) \end{bmatrix} \quad (\text{A.2})$$

The variables m_{abc} represent the instantaneous measurements of either phase to neutral voltages or line currents. The angular frequency ω in \mathbf{T}_+ is adopted as the same angular frequency of the grid. Moreover, the initial phase of the grid voltage between phase a and the neutral is adopted as zero, i.e., $v_a(t) = V \sin(\omega t)$.

The $dq_+ \mapsto abc$ transformation is given by (A.3), where the superscript T stands for transpose.

$$\begin{bmatrix} m_a(t) \\ m_b(t) \\ m_c(t) \end{bmatrix} = \mathbf{T}_+^T(t) \begin{bmatrix} m_d(t) \\ m_q(t) \end{bmatrix}. \quad (\text{A.3})$$

B. Negative Sequence Rotating Reference Frame

A measurement $[m_a \ m_b \ m_c]^T$ can be moved to the negative sequence RRF if the mid and right columns of \mathbf{T}_+ are swapped. The result is shown in (A.4). This RRF is denoted by dq_- in this paper. For the $abc \mapsto dq_-$ and $dq_- \mapsto abc$ transformations, replace \mathbf{T}_+ by \mathbf{T}_- in (A.2) and (A.3).

$$\mathbf{T}_- = \mathbf{T}_+ \begin{bmatrix} 1 & 0 & 0 \\ 0 & 0 & 1 \\ 0 & 1 & 0 \end{bmatrix} \quad (\text{A.4})$$

C. Negative ω Rotating Reference Frame

A measurement $[m_a \ m_b \ m_c]^T$ can be moved to the negative ω RRF if the sign of the angular speed in \mathbf{T}_+ is reversed. The result is shown in (A.5). This RRF is denoted by $dq_{-\omega}$ in this paper. For the $abc \mapsto dq_{-\omega}$ and $dq_{-\omega} \mapsto abc$ transformations, replace \mathbf{T}_+ by $\mathbf{T}_{-\omega}$ in (A.2) and (A.3).

$$\mathbf{T}_{-\omega} = \begin{bmatrix} -1 & 0 \\ 0 & 1 \end{bmatrix} \mathbf{T}_+ \begin{bmatrix} 1 & 0 & 0 \\ 0 & 0 & 1 \\ 0 & 1 & 0 \end{bmatrix} = \begin{bmatrix} -1 & 0 \\ 0 & 1 \end{bmatrix} \mathbf{T}_- \quad (\text{A.5})$$

APPENDIX B CASE STUDY DATA

TABLE B.I: Case study platform.

Parameter	Value	
System rated frequency	f_n	60 Hz
Generator rated apparent power		44 MVA
Gas turbine rated power		35 MW
Gen. and busbar rated ac voltage		11 kV
ESS rated apparent power	S_b	9.65 MVA
ESS HV ac rated voltage		11 kV
ESS LV ac rated voltage		690 V
ESS LV ac rated line current	I_b	8075 A
ESS LV base impedance	Z_b	0.049 337 Ω
LSC switching frequency	f_{sw}	2.5 kHz - 4 kHz
LSC dc voltage	U_{dc}	1200 V

TABLE B.II: Estimating a representative X/R .

Parameter	Value at (base) in pu		
		(88 MVA)	(9.65 MVA)
Transient reactance	x'_d	0.299	0.032 788
Stator resistance	r_s	0.0242	0.002 654
Breaker+HV devices res.	r_b	0.007 273	0.000 798
Load resistance	r_L	1.964	0.215 402
Transformer reactance	x_t	-	0.060
Transformer resistance	r_t	-	0.005
Capacitor impedance	x_c	-	20
Damping resistor	r_c	-	0.340 to 0.328
Main reactor resistance	r_r	-	0.01